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# A True Inline Coaxial-Cavity Filter with Two Symmetric Zeros

Stefano Tamiazzo, Giuseppe Macchiarella, *Fellow, IEEE*, Fabien Seyfert

**Abstract**— This work deals with the design of true inline filters with two symmetric transmission zeros. A new filters category named “path filters” is introduced (including the considered filters), his general features are discussed and analyzed and a general method for the synthesis of the low-pass prototype network is proposed. To validate the proposed design approach, a coaxial-cavity filter with a true inline topology exhibiting two symmetrical transmission zeros has been designed and fabricated. The realized prototype shows a response in good agreement with the theory.

**Index Terms**— inline filters, coaxial resonators, transmission zeros, prototype synthesis.

## I. INTRODUCTION

MOST applications of microwave filters in recent years are requiring increasingly compact, lightweight, and selective devices. For this reason, the research has focused on filters with simple topologies allowing the introduction of transmission zeros, even very close to the passband. As a result, many examples of filter realizations featuring the above characteristics have appeared in the literature, implemented in the most popular fabrication technologies [1]-[5].

A very convenient topological solution widely adopted since a long time is the inline configuration. As well know, this topology allows basically an all-pole characteristic, i.e., no transmission zeros can be introduced in the response. However, several variants of the basic configuration have been recently proposed, to allow the introduction of transmission zeros. It can be mentioned the configurations with frequency dependent couplings [6], some implementations of extracted-pole topology [7] and the use of strongly-coupled resonators [8]-[9]. However, all these solutions require a more or less marked deviation from the “true” inline configuration.

In this work we introduce a new class of filters, that we have called “path filters” (for the analogies with the family of path graphs [10]), featuring the true inline topology but with the source and load placed inside (instead of being the first and last node as in all pole filters). In general, this topology cannot be synthesized from the usual characteristic polynomials producing the generalized Chebycheff characteristic, unless further constraints on the derived polynomials are imposed. We have here defined the constraints allowing up to two imaginary

transmission zeros. Moreover, a procedure for the synthesis of the lowpass prototype has been developed, starting with the synthesis of the folded or transversal forms, followed by suitable matrix transformations.

Using the novel approach, the design and fabrication of a true inline filter of order 10 with two symmetric transmission zeros, has been carried out in coaxial technology. The realized prototype has been used to validate the design approach for path filters here proposed.

## II. THE “PATH FILTERS”

Fig. 1 shows the general configuration of path filters.

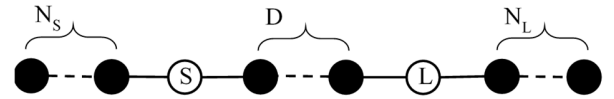


Fig. 1. General configuration of Path Filters. Each black node represents a resonator, the lines are the coupling inverters, the white nodes are the source and load.

This configuration is composed of three blocks of resonators, separated by source and load. The number of resonators before the source and after the load are  $N_s$  and  $N_l$  respectively, while the internal ones are  $D$ . The overall number of resonators is then  $N = N_s + D + N_l$ . We can observe that, for the minimum path rule [12], path filters allow introducing exactly  $M = N_s + N_l$  transmission zeros in the response.

In general, we can approach the synthesis of this filter class starting with the evaluation of the characteristic polynomials ( $F(s)$ ,  $P(s)$ ,  $E(s)$ ) determining the Generalized Chebycheff response in the normalized frequency domain  $s$  [11]. However, it can be shown that an additional constraint must be imposed on these polynomials. Assuming the filter response symmetric (i.e.  $S_{11} = S_{22}$ ) this constraint requires that each imposed transmission zero is also a double eigenvalue of the synthesized network. To demonstrate this requirement, let's start by the elements of ABCD and Z matrices of the filter, that can be expressed as polynomials ratios [11]:

$$\begin{aligned} A &= D = a(s)/P(s), \quad B = b(s)/P(s), \quad C = c(s)/P(s) \\ Z_{11} &= Z_{22} = a(s)/c(s), \quad Z_{12} = P(s)/c(s) \end{aligned} \quad (1)$$

Assume now that  $j\Omega_z$  is a root of  $P(s)$  (i.e., is a transmission zero). Due to the topology of the path filters, at the frequency

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of the zero a short circuit is produced in parallel to source and load ( $Z_{11}=Z_{22}=0$ ). Consequently,  $a(j\Omega_z)=0$  and  $c(j\Omega_z)\neq 0$ . Moreover, the assumed lossless condition requires the determinant of ABCD matrix equal to 1, that is:

$$a^2(s) - P^2(s) = b(s)c(s) \quad (2)$$

From (2) descends that  $j\Omega_z$  must also be a double root of  $b(s)$ . As the roots of  $b(s)$  are also the eigenvalues of the filter shunt model [11], we have demonstrated that every transmission zero of a symmetric path filter, synthesized with shunt equivalent resonators, must also be a double eigenvalue of the filter equivalent circuit. Note that, being the eigenvalues of a lossless filter imaginary, also the transmission zeros introduced by path filters must be imaginary, as above assumed. Moreover, being  $N_z = N_S + N_L$  the number of double eigenvalues,  $N > 2N_z$  implies that  $D \geq N_S + N_L$ .

From what has been said above, the synthesis of path filters with Chebycheff (quiripple) response requires an additional constraint (for each transmission zero), in addition to those defining the usual filter specifications. Unfortunately, no degree of freedom is available after the requirements have been set, so we must give up assigning one of them to make the synthesis of path filters possible. In this work we have used the return loss parameter to get the characteristic polynomials of path filters exhibiting a symmetric response with two zeros ( $\pm j\Omega_z$ ). Note that, in this case,  $N_S + N_L \leq 2$  (the zeros can be extracted both at source (load) side or one at source and one at load).

#### A. Polynomials Evaluation

As pointed out above, the condition for synthesizing a path prototype is to have eigenvalues of multiplicity 2 in correspondence of each assigned pair of symmetric transmission zero. However, this condition is in general not satisfied if the characteristic polynomials are computed with the classical methods [10]. We have then developed an empirical procedure that, although not formally proven, has been assessed on the base of several examples up to  $N_S + N_L = 2$ . It consists of the following steps:

- Assign the filter order and the desired transmission zeros (imaginary)
- Evaluate the reflection characteristic polynomial  $F(s)$
- Compute the filter eigenvalues (represented by the roots of the denominator polynomial of the filter admittance matrix) as function of the leading coefficient  $p_0$  of the transmission polynomial  $P(s)$
- Select the value of  $p_0$  producing two coincident eigenvalues at the frequencies of the transmission zeros.

Once  $p_0$  has been determined, all the characteristic polynomials are defined. However, as observed before, the return loss cannot be assigned freely because it depends on  $p_0$ . The not assignable return loss level represents the main drawback of the proposed procedure. We note however that in case the assigned transmission zeros are relatively close to the passband, the resulting level of return loss is generally acceptable. Fig. 2 gives an idea of the return loss obtained for three values of the assigned transmission zeros and  $N$  varying from 5 to 15. It can be observed that RL is little dependent on  $N$  and increases by moving the transmission zeros away from the passband.

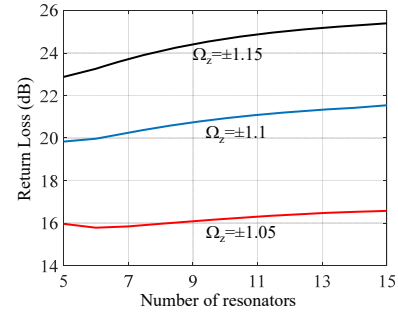


Fig. 2. Return Loss obtained from the computed polynomials for three different assignment of the transmission zeros and  $N$  ranging from 5 to 15.

#### B. Synthesis of the path prototype

In line of principle, the synthesis of the path prototype could be approached with the evaluation of the transversal prototype, followed by suitable matrix transformations. Unfortunately, the transversal form of filters with double eigenvalues cannot be synthesized using the classical method given in the literature [13], which holds only for networks with simple eigenvalues. We have then used the folded canonical form as initial prototype [11], which can be synthesized using the extractions method [14], not based on the eigenvalues computation. The coupling matrix of the folded prototype is then suitably reconfigured to get the coupling matrix of the path filter in Fig. 1. To this end, first the conversion to the Wheel form is carried out using the algorithm in [15]. Then a sequence of matrix rotations is applied, to get out a triplet form from the load and moving it up to the source (the same technique used in [15]). When the triplet arrives in the final position, all cross couplings disappear, and the "path" topology is obtained.

### III. FILTER DESIGN

The filter to be designed has the following electrical requirements:

- Passband: 3394-3806 MHz, Return Loss  $\geq 18$  dB
- Order (number of resonators): 10
- Stopband attenuation:  $>30$  dB for  $|f-f_0| > 230$  MHz

To fit the attenuation requirements two transmission zeros must be placed symmetrically above and below the passband at 3835 MHz and 3368.3 MHz. Note that the rejection actually presented by the synthesized path filter depends on the resulting return loss, that cannot be assigned a priori. At the end of the polynomials evaluation, the fulfillment of the above requirements must then be verified before proceeding with the synthesis of the prototype.

The reflection zeros defining the monic polynomial  $F(s)$  are first evaluated from the normalized transmission zeros ( $\pm j1.13268$ ):  $zF = [0.9917, 0.9194, 0.7562, 0.4994, 0.1747, -0.9917, -0.9194, -0.7562, -0.4994, -0.1747]$ . The polynomial  $P(s)$  is defined as function of the unknown highest degree coefficient  $p_0$ :  $P(s) = p_0(s^2 + 1.283)$ . Finally, the polynomial  $E(s)$  defining the filter poles can be computed by spectral factorization from the Feldtkeller equation (lossless condition) [11]:  $E(s)E^*(s) = P(s)P^*(s) + F(s)F^*(s)$ . The filter eigenvalues are the roots of polynomial  $b(s)$  which can be evaluated from the characteristic polynomials as described in [11]. We can then represent the eigenvalues as

function of the real parameter  $p_0$  (Fig. 3). It can be observed that two pairs of symmetrical eigenvalues cross for  $p_0=0.041803$ .

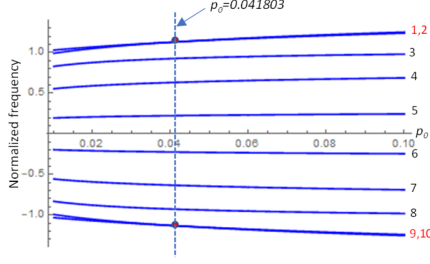


Fig. 3. Computed filter eigenvalues as function of  $p_0$ .

Moreover, at the crossing points the eigenvalues coincide with the assigned transmission zeros ( $\pm 1.13268$ ). For the computed value of  $p_0$  the return loss is 23.4407 dB and the condition for implementing the filter with the path topology is satisfied. The response in the normalized domain is shown in Fig. 4. It can be observed that return loss is larger than 18 dB while attenuation in the stopbands exceeds 30 dB. The filter requirements are then satisfied, and it is possible to proceed with the synthesis of the path filter.

We have assumed  $N_S=2$  and  $N_L=0$ . The synthesis of the prototype is carried out with the procedure described before obtaining the normalized coupling matrix of the desired path filter:  $M_{i,i}=0$ ,  $M_{s2}=0.67$ ,  $M_{s3}=0.802$ ,  $M_{12}=1.133$ ,  $M_{23}=0$ ,  $M_{34}=0.604$ ,  $M_{45}=0.526$ ,  $M_{56}=0.525$ ,  $M_{67}=0.531$ ,  $M_{78}=0.545$ ,  $M_{89}=0.596$ ,  $M_{910}=0.862$ ,  $M_{10L}=1.046$ .

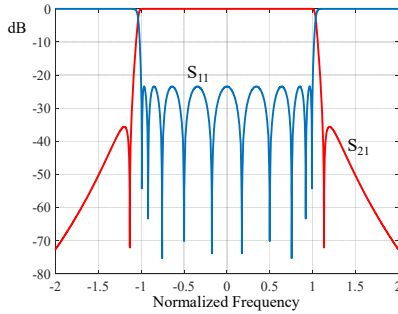


Fig. 4. Computed polynomial response of the normalized prototype with  $p_0=0.041803$  (RL=23.4407 dB)

The last step of the synthesis is the de-normalization of the normalized prototype defined by the computed coupling matrix. In this step we determine the coupling coefficients and the resonating frequencies of the filter in the bandpass domain (Fig. 5), that are used for dimensioning the physical structure implementing the filter.

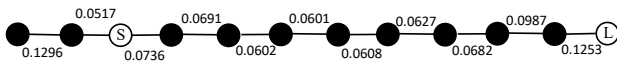


Fig. 5. De-normalized equivalent circuit of the path filter. Black circles represent the resonators (all resonating at  $f_0=3594.1$  MHz). The numbers above or below the solid lines are the coupling coefficients between the resonators.

For the physical realization of the filter (Fig. 6), a comb structure inside a box of height 19 mm has been employed. The coupled resonators are square cylinders of size 3.5 mm x 3.5

mm and of various heights (averaging 18 mm). The quality factor of the fundamental resonant mode (3.6 GHz) is about 2500 and adjacent rods are coupled by proximity and possibly connected by a thin metal bar in places where strong couplings are required. All input and output couplings (three in this case, two at the source end and one at the load end) are realized through suitable lengths of transmission (strip) lines soldered to the rods 2, 3 and 10 (Fig. 6), at a suitable distance from the base (ground plane).

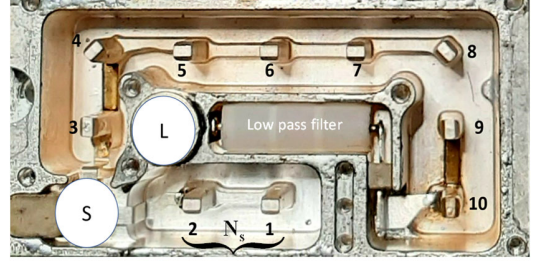


Fig. 6. Fabricated structure of the path filter. The resonators are the numbered square cylinders (1 and 2 are those realizing the transmission zeros).

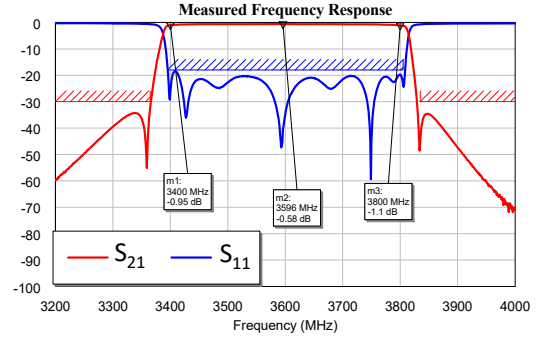


Fig. 7. Measured response of the fabricated prototype.

Fig. 7 shows the measured response of the realized prototype. Although the agreement with the polynomial response of Fig. 4 is good, the limited range and resolution of the adopted tuning elements prevented from a better 'shaping' of the return loss curve.

#### IV. CONCLUSION

In this paper an introduction to the design of a class of true in line filters with up two symmetric transmission zeros has been given, along with a practical realization in the 3.4 – 3.8 GHz band. This class of filters appears to be promising for the realization of symmetrical frequency responses usually required in TDD radios for cellular networks operating in that range of frequencies. Compared to the canonical cross coupled alternatives, there is no need in path filters to implement negative couplings, usually associated with spurious resonances and tolerance issues. Finally, it must be emphasized that the design approach proposed here represents the first analytical solution for the class of filters considered. Indeed, previous works dealing with this topology [16] address the synthesis of the low-pass prototype using optimization techniques. We are currently working on the extension of the path filters synthesis to a larger number of transmission zeros (not necessarily symmetric).

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