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Experimental Demonstration of Real Time Receiver for FDMA PON

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Abstract FDMA PON provides high aggregate capacity (20-40Gbps) without requiring the user modules to operate at such high data rate. In this paper, we present for the first time a real time implementation of a FDM receiver in FPGA 1Gbitps in transceiver modules for an ONU and OLT.

Introduction
In order to meet the growing demand for data rate over Passive Optical access Networks (PON), TWDM PON has been selected for NG-PON2 with capacity of 40Gbps downstream (DS) and 10Gbps upstream(1)[2] (US). Although highly performing, this solution presents several disadvantages arising from the necessity to use four wavelength pairs to carry the traffic with potential cross channel interferences (e.g. rogue Optical Network Unit – ONU) and the necessity to use very high performance transceivers at the customer premises including wavelength tunability and high clock rate (10Gbps/2.5Gbps) which is source of cost and large power consumption[3]. Frequency Division Multiple Access (FDMA) PON is an alternative to this solution that has been demonstrated to be able to carry 32Gbps DS[7] and also 32Gbps US[8] on a single wavelength pair, managed from the Optical Line Terminal (OLT) side. Also, FDMA PON ONU can be integrated fully in Silicon[9] to decrease cost. We also demonstrated that the RF and electronic hardware necessary to allow transmission over the FDMA PON is equivalent to a simple, low cost, Ultra Wide Band (UWB) transceiver[10]. However the useful data rate achieved by the UWB transceiver was at maximum 480Mbps.

In this paper we experimentally demonstrate, for the first time, the real time implementation of a Frequency Division Multiplexing (FDM) receiver in Field Programmable Gate Array (FPGA) using a dual input Analogue to Digital Converter (ADC) operating at 1GS/s to receive and demodulate Quadrature Phase Shift Keying (QPSK) signals carrying 1Gbps. We have successfully tested this real time receiver in the Downstream (DS) i.e. at the ONU side and in the Upstream (US) i.e. at the OLT side. We report results of Bit Error Rate (BER) measurement as a function of RF carrier frequency and optical budget (OB) between the OLT and ONU.

Digital Signal Processing
The Digital Signal Processing implemented in this paper is presented Fig.1. The received analogue signal is sampled at 1 GSp/s by a pair of 10 bits resolution ADC, giving In-phase(I) and Quadrature phase(Q) digital signals. Both of them are then de-serialized to match the FPGA clock at 250MHz. An IQ compensator corrects the unbalanced default from optical and RF sub-system. An eleven taps T/2-fractionaly spaced adaptive equalizer, based on Least Mean Square (LMS) error, is used to compensate the channel intersymbol interference and the carrier frequency offset. Due to the sampling rate higher than the FPGA processing frequency, algorithms are computed by a full pipelined parallel architecture. Thereby, two processing units compute input data. This architecture is easily scalable for higher sampling rate frequency ratio. Two T/2-adaptive equalizers compute two consecutive symbols. The coefficients are identical for both filters and are updated at each FPGA cycle for maximal sampling and carrier frequency offset tolerance. Instead of classic solutions combining Gardner[5][6] and a frequency recovery loop for the sampling frequency offset (SFO) compensation, a smart implementable solution using center-tap tracking algorithm[4] is implemented. This algorithm analyses the filters coefficients magnitudes and operates a
coefficient shift to keep the maximum energy on
the central coefficient. If the TX sampling
frequency is greater than the RX one,
coefficients are shifted to the left and an
additional symbol has to be computed
compensating the temporal output shift. This is
done through a dedicated third filter.
Reciprocally, in the case of right shift, a
redundant symbol is removed from the output
stream.
Due to irregular data flow at the output of the
decisions blocks, data are memorized in a First
In First Out (FIFO) buffer. An FPGA internal
Phase Locked Loop (PLL), controlled by FIFO
filling, creates an image of the TX clock.
Boards used are FMC126 (FPGA Mezzanine
Card) from 4DSP for the ADCs, VC707 from
Xilinx for FPGA and HMC821 from Hittite for the
sampling clock.
Tab. 1 highlights implementation results
showing main FPGA resources usage. Although
this study was performance oriented, it’s
noticeable that few DSP resources (multipliers)
are used.
Tab. 1: Ressources usage for Filter+LMS+ SFO+ décision

<table>
<thead>
<tr>
<th>Resource</th>
<th>Number of resources</th>
</tr>
</thead>
<tbody>
<tr>
<td>DSP</td>
<td>143</td>
</tr>
<tr>
<td>Flip Flop</td>
<td>9484</td>
</tr>
<tr>
<td>LUT</td>
<td>5526</td>
</tr>
</tbody>
</table>

As described in Fig. 1, we propose a simple
non-data aided (or unsupervised) transmission
system because of its implementation efficiency
and its ability to be scalable for higher sampling
rates. We can notice that FMC126 supports
2GSps hence the proposed system can be
easily upgraded for operating at 2GSps while
keeping the same hardware configuration.

Fig. 2: B2B electric, error rate with phase rotation

After processing by FPGA, the I/Q signals are
analysed by a BER tester. The 1Gbit/s QPSK
signal used for measurement is generated with
an 8GSps Arbitrary Waveform Generator
(AWG). In first step, we have tested the
tolerance of our receiver to Carrier Frequency
Offset (CFO) which is numerically generated
and played by AWG. On Fig. 2, the CFO
tolerance is greater than 100kHz with 9dB of
SNR and 180kHz without noise at error free.

System assessment
Our experimental set-up, equivalent to the one
presented in\cite{7,8} is representative of a fully
loaded 64 split class B+ PON.
The test RF signal is produced by the set of two
AWG. The first AWG has two outputs with
1GSp/s, generating the QPSK baseband data
with 500Mbps each and feeding the input of an
IQ mixer. The RF Local Oscillator is obtained
from a Frequency Synthesiser and can be tuned
from 2 to 18GHz. The signal outputting the IQ
mixer is called the “user signal” and is the one
over which we measure the BER. The second
AWG has 24GS/s capability and generates 11
dummy neighbouring RF channels around the
users signal in order to simulate the presence of
other users. This “complementary” signal
occupies a bandwidth from 2 to 12GHz at
maximum. A guard band of 20MHz is
maintained each side of the user signal. The
light is then amplified by an Erbium Doped Fibre
Amplifier (EDFA) for an optical output power of
+12dBm. To simulate a Passive Optical Network
(PON) we use Standard Single Mode Fibre
(SMF) spool (25 km long) and a Variable Optical
Attenuator (VOA). A polarization scrambler is
also used to make the set-up more realistic.
Finally the light is photo-detected by a PIN
photodiode with 7 GHz bandwidth and a
responsivity of 0.8 A/W followed by a TIA. Then
the signal inputs the receiver IQ mixer and
ADC/FPGA board. The resulting BER is
measured directly from the FPGA.
US Set-up (Fig. 4): An ECL is used to serve as
LO in a coherent receiver and seed source for
the reflective FDMA ONU. The launch power
into the PON is set to +12dBm. The PON itself is
made of a polarization scrambler followed by a
3dB optical coupler. After the coupler, two
branches are considered. The first branch is
made of a VOA, a 25km spool of SMF and
reaches ONU1 whose structure is similar to the
one reported in reference document\cite{8}. Using the
VOA, we can simulate optical budgets ranging
from 16dB to over 40dB as required. The
second branch of the PON is made of another 3dB optical coupler. One branch is connected to a second ONU (denoted ONUx) while the other is connected to an EDFA used as Amplified Spontaneous Emission (ASE) source used to load the system with optical noise equivalent to the presence of 64 active ONUs on the PON tree. ONU1 is modulated with a single user signal while ONUx is modulated with the complementary signal. At the OLT side, two RF signals are obtained from the coherent receiver as it is single polarization\[^7\]. These signals are combined to produce another two signals containing the baseband data for the user signal under test\[^10\] which can be used to feed directly the two 1GS/s ADC and FPGA where the BER is measured.

**Results**

Results are displayed in Fig. and Fig. . In the DS, it is possible to obtain a BER<10\(^{-3}\) up to 34dB of OB for the lowest frequency channel. Also, a BER of 10\(^{-3}\) could be obtained up to the channel whose centre frequency is 9GHz. In the US, an OB of 34dB is also demonstrated for the lowest frequency channel for BER<10\(^{-3}\) while the last channel for which we can obtain a BER<10\(^{-3}\) is at 8GHz. Note that the limitations observed in these experiments rather come from the RF IQ mixers used and the roll-off of the frequency responses of the photodetectors and amplifiers rather than from the FDM receiver itself which operates purely in base-band.

**Conclusions**

For the first time, we have demonstrated in real-time the feasibility of a FDMA PON receiver at 1 Gbit/s for access network. We have developed transceiver modules for next generation PON systems that achieve smart implementable solution of the main digital signal processing functions.

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**References**